Low-Sensitivity Active-RC Filters Using Impedance Tapering of Symmetrical Bridged-T and Twin-T Networks

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Abstract— **In this paper we introduce a new design procedure for low-sensitivity filter sections, which have a symmetrical passive-RC network in the operational amplifier (opamp) feedback loop. In the design procedure we apply impedance scaling to the symmetrical bridged-T and twin-T networks; they become "potentially symmetrical" [1]. The design of low-sensitivity allpole active-RC filters, which have an RC-ladder network in the opamp feedback loop, has already been published [2]. There, successive L-sections of the ladder structure are impedance scaled upwards, from the driving source to the positive opamp input; we refer to it as "impedance tapering". In both cases we reduce the filter's magnitude sensitivity to variations of the passive components of a circuit. The new design concept will be demonstrated by designing two very popular and often used filter sections: a band-pass realized by the Deliyannis SAB, and a band-rejection filter with a Twin-T. The sensitivity analysis is examined analytically and double-checked using PSpice Monte Carlo runs.**

I. Introduction

In this paper we present a low-sensitivity design procedure for two very often-used 2nd-order active-RC single-opamp filter sections. One is used for the realization of a band-pass (BP) transfer function and is known as a Deliyannis section. It is realized by a bridged-T RC-network in the negative feedback loop and belongs to "class-3" networks [3]. The other is a band-rejection (BR) section with a Twin-T RC-network in the positive feedback loop and belongs to the "class-4". Both are described in [1][4] and are based on physically symmetrical passive RC networks. The newly introduced design concept reduces the sensitivity to the passive components of the circuit of those two filter sections, making them even more attractive for the realization of filter circuits. In the new design procedure, the topology and component count remain the same, we just judiciously select the component values, in order to decrease the component tolerance sensitivity.

The design method is based on impedance scaling of one half of a symmetrical passive RC-network, in order to maximize its pole Q factor. It is well known that the pole Q, $\hat{q}$ of a passive RC network is upper limited with the value of (never accessible) 0.5; if we want to reach it we will need to realize an infinite ratio of two components [1]. Note, that we use the symbol "^" on the top of any passive-network parameter. Design of the passive RC network such that its pole Q is as close to 0.5 as possible, is very valuable due to several reasons presented in [4] (pp. 315-339).

II. Selectivity of Passive RC Networks

One very useful network characteristic in connection with RC networks is that of symmetry. It is well known that physically and electrically symmetrical networks (and reciprocal—this property is *generally* fulfilled for passive networks ['generally' because it does not hold for the 'passive' gyrator, for example]), can be split into two identical halves. Then, we can apply Bartlett's bisection theorem to readily calculate open-circuit impedances [1].

The process of deriving a so-called "potentially symmetrical" bridged-T network is shown in Fig. 1 if we scale the impedance of one half of the network (e.g. right) by a constant factor ρ. The transfer function of the bridged-T in Fig. 1 is given by [1][4]:

$$\hat{t}_{32}(s)=\frac{V_2}{V_3}=k_{32}\frac{s^2+(\omega_z/q_z)\cdot s+\omega_z^2}{s^2+(\omega_p/\hat{q})\cdot s+\omega_0^2}, \qquad (1)$$

where $k_{32}=1$, $\omega_0=\omega_z$, $\hat{q}<q_z$ and

$$\omega_0=\frac{1}{\sqrt{R_1R_2C_1C_2}};\; q_z=\frac{\sqrt{R_1R_2C_1C_2}}{R_1(C_1+C_2)};\; \hat{q}=\frac{\sqrt{R_1R_2C_1C_2}}{R_1(C_1+C_2)+R_2C_2}. \qquad (2)$$

The transfer function in (1) has the characteristic of the "Frequency Rejection Network" (FRN) [1][3]. For the "symmetrical" bridged-T in Fig. 1(a) we have:

$$\omega_z=\omega_0=(RC)^{-1};\; q_z=1;\; \hat{q}=1/3. \qquad (3)$$

Deriving the "potentially symmetrical" bridged-T as shown in Fig. 1(d), we obtain the same values for ω_z and q_z as in (3), but for the pole Q, $\hat{q}$ we obtain:

$$\hat{q}_{\text{Bridged-T}}=\rho/(1+2\rho)\big|_{\rho\to\infty}=0.5\,. \qquad (4)$$

It is apparent from (4) that by increasing the impedance-scaling factor ρ the passive pole Q, $\hat{q}$ is increased towards 0.5. In what follows, we shall demonstrate the reduction of sensitivity when increasing the ρ, in the class-3 and class-4 filters, separately.

III. Class-3 Filters—Negative Feedback

Consider a common 2nd-order class-3 active-RC filter section with BP characteristic shown in Fig. 2. It is known as the Deliyannis section [3], and is suitable for realization of medium-Q values ($2<q_p<20$) [5]. The circuit in Fig. 2 has the same bridged-T network as in Fig. 1, providing FRN characteristic in the negative feedback loop (from node 3 to 2), while in the signal forward path (node 1 to 2) it has a BP RC ladder network. Because of the latter, its overall BP transfer function is given by:

$$T(s)=\frac{V_{out}}{V_{in}}=\frac{Ka_1s}{s^2+a_1s+a_0}=\frac{K\cdot(\omega_p/q_p)\cdot s}{s^2+(\omega_p/q_p)\cdot s+\omega_p^2}, \qquad (5)$$

where the pole frequency, ω_p and pole Q, q_p (or the transfer function coefficients $a_1=\omega_p/q_p$ and $a_0=\omega_p^2$) are given by:

$$K=q_p\overline{\beta}\sqrt{\frac{R_2C_2}{R_1C_1}};\; \omega_p=\frac{1}{\sqrt{R_1R_2C_1C_2}};\; q_p=\frac{\sqrt{R_1R_2C_1C_2}}{R_1(C_1+C_2)+R_2C_2(1-\overline{\beta})}, \qquad (6)$$

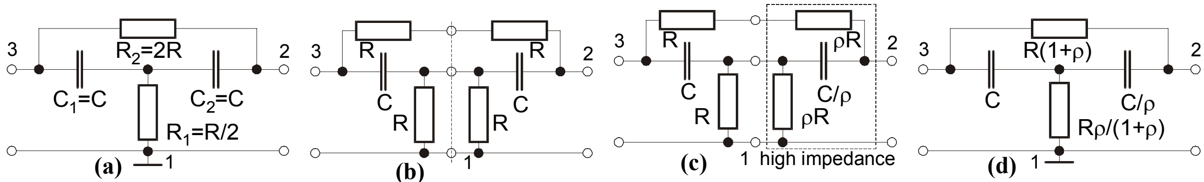

Figure 1. Bridged-T network. **(a)** Common configuration. **(b)** Broken up symmetrically. **(c)** Impedance scaled. **(d)** Potentially symmetrical.

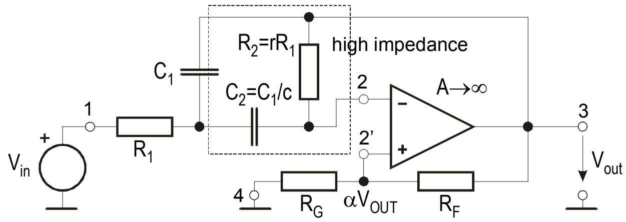

Figure 2. 2[nd]-order BP active-RC filter (Deliyannis SAB section) with general scaling factors r and c as in [6].

and where $\bar{\beta}=1+R_G/R_F$ (7)

represents a positive feedback gain, realized by resistors R_G and R_F. A positive feedback in the circuit, is represented by a direct measure $\alpha=R_G/(R_F+R_G)$; $0<\alpha<1$ in Fig. 2 (node 3 to 2').

The complementary transformation between class-3 network with additional positive feedback and class-4 network is demonstrated in [3] (p. 167) and [7]. In [7] it was shown that a 2[nd]-order class-4 high-pass (HP) filter and class-3 BP filter as shown in Fig. 2, are related by the complementary transformation, and the low-sensitivity design of one will produce the low-sensitivity design of the other filter; their coefficient-to-component sensitivities also have the same form. It is more practical to use $\bar{\beta}=(1-\alpha)^{-1}$; $0<\bar{\beta}<\infty$ instead of α, because the equations for pole parameters as functions of components (6) are then identical for both filters [6]. Note that the class-4 (HP) circuit has the gain $\beta=1+R_F/R_G$ instead of gain $\bar{\beta}$; the gains are related by $1/\bar{\beta}+1/\beta=1$ [7]. Sensitivity of coefficient a_0 to all components is -1, thus only the sensitivities of a_1 are presented in the first column of Table 1. Note that all sensitivities in Table 1 are proportional to pole Q, q_p.

Example: Consider BP and BR filters having 1kHz center frequency and pass-band range of 200Hz. To obtain this selectivity we need the pole Q factor of $q_p=\omega_0/B=5$, and the active-RC filter realization. Magnitudes of the transfer function characteristics are shown in Fig. 3.

One segment of the sensitivity analysis (given in [6]) of the SAB filter in Fig. 2 will be summarized here. Filters with various resistance (r) and capacitance (c) ratios are presented Table 2. In the last two columns the Q-values of the bridged-T network calculated

TABLE I. SENSITIVITY OF COEFFICIENT a_1 TO COMPONENT VARIATIONS IN A 2[ND]-ORDER BAND-PASS FILTER.

x	$-(1/q_p)\cdot S_x^{a_1}$		
R_1	$-\sqrt{\frac{R_2C_2}{R_1C_1}}\cdot(\bar{\beta}-1)$	$-\frac{1+\rho}{\rho}(\bar{\beta}-1)$	-0.8
R_2	$\sqrt{\frac{R_1C_1}{R_2C_2}}+\sqrt{\frac{R_1C_2}{R_2C_1}}$	1	1
C_1	$\sqrt{\frac{R_1C_2}{R_2C_1}}-\sqrt{\frac{R_2C_2}{R_1C_1}}(\bar{\beta}-1)$	$(1+1/\rho)(1-\bar{\beta})+$ $+1/(1+\rho)$	$-0.8+\frac{1}{1+\rho}$
C_2	$\sqrt{\frac{R_1C_1}{R_2C_2}}$	$\frac{\rho}{1+\rho}$	$\frac{\rho}{1+\rho}$

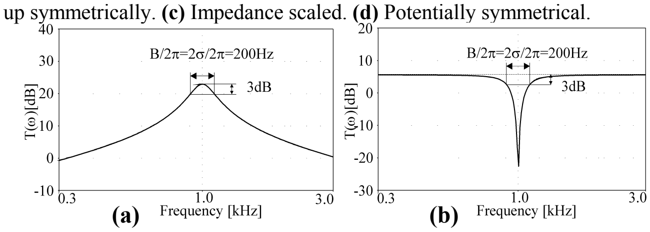

Figure 3. The 2[nd]-order filter transfer function magnitude with f_0=1kHz, q_p=5. **(a)** Band-pass. **(b)** Band-rejection.

from (2) are given. Corresponding Monte Carlo (MC) runs with 1% Gaussian distribution, zero-mean resistors and capacitors were carried out and presented in Fig. 4. It is obvious, for the reasons given in [6] that filter no. 4 with equal capacitors and impedance scaled resistors has min. sensitivity.

When used in the "infinite-gain" mode the closed-loop poles in (5) of the class-3 network coincide with the open-loop zeros of bridged-T in (1). By applying an additional positive feedback the closed-loop poles move closer to the jω-axis, starting from the zeros of the bridged-T. Therefore, from (2) and (6) we have the relationship for pole Q, q_p, which is given by ([3] p. 161):

$$q_p=\hat{q}[1-\bar{\beta}(1-\hat{q}/q_z)]^{-1};\quad \hat{q}<q_z\le q_p\,. \tag{8}$$

From (8) obviously, the pole Q, q_p has the form:

$$q_p=\kappa_1\cdot(\kappa_2-\bar{\beta}\kappa_3)^{-1}, \tag{9}$$

where κ_1, κ_2, and κ_3 depend only on the passive RC network [2]. Calculating the relative sensitivity of the pole Q, q_p to the variations of positive feedback gain $\bar{\beta}$, we obtain [1][2]:

$$S_{\bar{\beta}}^{q_p}=-S_{\bar{\beta}}^{a_1}=q_p/\hat{q}-1\,. \tag{10}$$

TABLE II. COMPONENT VALUES OF 2[ND]-ORDER BP FILTERS WITH VARIOUS SCALING FACTORS (RESISTORS IN [KΩ], CAPACITORS IN [NF]).

No.	r	c	R_1	C_1	R_2	C_2	$\bar{\beta}$	$\hat{q}$	q_z
1)	1	1	15.9	10	15.9	10	2.8	0.33	0.5
2)	4	4	15.9	10	63.6	2.5	2.05	0.44	0.8
3)	1	4	31.8	10	31.8	2.5	5.6	0.33	0.4
4)	4	1	7.96	10	31.8	10	1.4	0.33	1.0

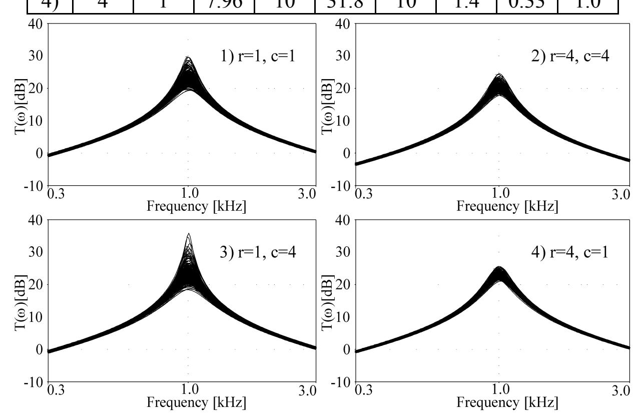

Figure 4. Monte Carlo runs of impedance-tapered 2[nd]-order BP filters given in Table 2.

Note that pole Q, q_p sensitivity to gain variation is reduced as the value of the passive pole Q, $\hat{q}$ increases. Will the decrease of sensitivity in (10) really reduce the sensitivity to the tolerances of the two positive-feedback resistors R_G and R_F? The relative variation of pole Q, q_p, due to variations of resistors R_F and R_G, is given by:

$$\frac{\Delta q_p}{q_p} = S_{\bar{\beta}}^{q_p} \cdot \frac{\Delta \bar{\beta}}{\bar{\beta}}; \text{ where } \frac{\Delta \bar{\beta}}{\bar{\beta}} = S_{R_G}^{\bar{\beta}} \frac{\Delta R_G}{R_G} + S_{R_F}^{\bar{\beta}} \frac{\Delta R_F}{R_F}. \quad (11)$$

From (7) we can readily calculate (in class-3) the sensitivity of the gain $\bar{\beta}$ to the feedback resistors R_F and R_G:

$$S_{R_G}^{\bar{\beta}} = -S_{R_F}^{\bar{\beta}} = 1 - 1/\bar{\beta}. \quad (12)$$

Expressing $\bar{\beta}$ from (8), and substituting it into (12) and with (11) we have:

$$S_{R_G}^{q_p} = -S_{R_F}^{q_p} = S_{\bar{\beta}}^{q_p} \cdot S_{R_G}^{\bar{\beta}} = q_p / q_z - 1. \quad (13)$$

Note that the q_p sensitivities to resistors R_G and R_F in (13) are *independent* of passive pole Q, $\hat{q}$ value (the term $q_p/\hat{q}$ -1 has cancelled out). Furthermore, the sensitivities in (13) are inversely proportional to the q_z. Thus to reduce it, we should use large q_z values (note that filter no. 4 with min. sensitivity has largest q_z in Table 2). From (2) it is obvious that for large q_z we must let C_1=C_2 and $R_2/R_1=4q_z^2$ (large resistor spread is required). It is known [1] that by bridged-T $\hat{q}$ and q_z are not independent. They cannot reach their respective max. values at the same time; the larger q_z is selected, the smaller $\hat{q}$ becomes. If we want to reduce the sensitivity of the circuit in Fig. 2 as much as possible, we reach the case when there is no positive feedback at all (q_p=q_z, $\bar{\beta}$=1, $R_2/R_1=4q_p^2$!). The "medium-Q" circuit in Fig. 2, then simplifies into "low-Q" circuit ($\bar{\beta}$=1) as defined in [5]. It provides a good solution when pole Q is smaller than 2. "Low-Q" circuit is not suitable for larger pole Q realizations because its component spread and the gain-sensitivity-product (GSP)† are both proportional to q_p^2. By "medium-Q" filter ($\bar{\beta}$>1) the GSP is proportional to q_p and the component spread is not so critical [5].

In the new design instead of general scaling factors *r* and *c* in Fig. 2 we introduce scaling factor ρ as in Fig. 1(d) to calculate elements of potentially symmetrical bridged-T, using:

$$R_1=\rho/(1+\rho)R;\ C_1=C;\ R_2=(1+\rho)R;\ C_2=C/\rho. \quad (14)$$

With (14) we obtain the sensitivity relations given in the second column of Table 1. With $\bar{\beta}$ from (8), and with (3), (4) and (14) for the potentially symmetrical bridged-T we have:

$$\bar{\beta} = 1 + (1 - q_p^{-1}) \cdot \rho/(1+\rho) \quad (15)$$

Substituting (15) into the second column of Table 1, we obtain the sensitivities in its last column (in our example of q_p=5 the term ($1-q_p^{-1}$) in (15) equals 0.8). Obviously, only the sensitivities to C_1 and C_2 are dependent on the factor ρ and they worsen as ρ (i.e. the value of $\hat{q}$) increase. From (13) we have $S_{R_{G,F}}^{q_p}$ =±4.

To double-check the above conclusions we designed the filter in Fig. 2, with two values of ρ. The component values of the resulting filters are in Table 3, and MC runs are in Fig. 5. It appears that as ρ increases, the sensitivities in Fig. 5 are getting slightly worse. Thus, lower sensitivity of the two has the filter no. 1) which has ρ=1 and a symmetrical bridged-T network. Incidentally it is the identical filter to the filter no. 4) with min. sensitivity in Table 2 (and in [6]). Obviously, here tapering with potentially symmetrical bridged-T does not help. In [5] are given design procedures for min.-GSP biquads. In most of the circuits in [5], one additional degree of freedom is available, which permits to choose the values and ratios of two (or three) components. The optimum trade-off in the Deliyannis circuit between q_z (neg. feedback) and $\bar{\beta}$ (pos. feedback) is to choose resistor ratio R_2/R_1>1 (by which the q_z is increased) thus reducing passive sensitivity, and to calculate capacitor ratio C_1/C_2 for min. GSP (from [5] p. 54), which provides circuit with reduced active sensitivity, as well.

† The GSP gives a measure of a filter's magnitude sensitivity to the open-loop gain (*A*) variation of the active component [5].

TABLE III. COMPONENT VALUES OF 2ND-ORDER BP FILTERS WITH POTENTIALLY SYMMETRICAL BRIDGED T.

No.	ρ	R_1	C_1	R_2	C_2	$\bar{\beta}$	$\hat{q}$	q_z
1)	1	7.96	10	31.8	10	1.4	0.33	1.0
2)	4	12.7	10	79.6	2.5	1.64	0.44	1.0

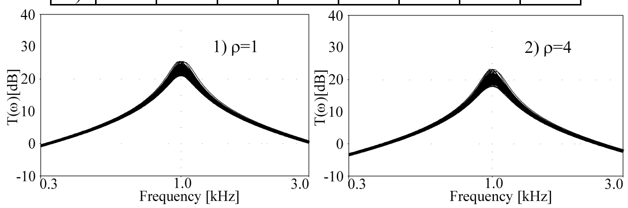

Figure 5. Monte Carlo runs of impedance-tapered 2nd-order BP filters given in Table 3.

IV. CLASS-4 FILTERS—POSITIVE FEEDBACK

As a representative example consider a 2nd-order class-4 BR (or notch) filter shown in Fig. 6, which is known as "Split-Feedback FRN" (SF-FRN) [3]. It is suitable for medium-Q realizations [5]. It has a potentially symmetrical "Twin-T" circuit in the positive feedback loop (inside rectangle) [1]. In [3] (pp. 224-229) the "Standard" FRN (ST-FRN) is presented, which has feedback on both R_3 and C_3 legs (switch S_1 is in the position "ST-FRN"). To make possible the realization of finite pole-Q, q_p ST-FRN needs a "loading network" of twin-T as in Fig. 6 [3]. In what follows we shall concentrate on SF-FRN because it is much simpler. It can readily be shown that the design techniques and results obtained for SF-FRN can be applied for the design of low-sensitivity ST-FRN, and for all-pass (AP) networks in [3], as well.

The transfer function is given by:

$$T(s) = \frac{V_{out}}{V_{in}} = K \frac{s^2 + \omega_z^2}{s^2 + (\omega_p / q_p) \cdot s + \omega_p^2}. \quad (16)$$

The parameters in (16) are given by [3]:

$$K=\beta;\ \omega_p^2 = \omega_z^2 = \frac{1}{R_1 R_2 C_s C_3} = \frac{1}{C_1 C_2 R_s R_3};\ q_p = \frac{R_2 C_1}{C_2 R_s + C_s R_1 (1-\beta)}, \quad (17)$$

where $\beta = 1 + R_F/R_G$ (18)

is the positive feedback gain in the class-4 circuits and

$$C_s=C_1C_2/(C_1+C_2),\ R_s=R_1+R_2,\ R_p=R_1R_2/(R_1+R_2),\ C_p= C_1+C_2. \quad (19)$$

Note also that $q_z=\infty$, if the "balance condition" for the Twin-T network holds, and it is given by [1]:

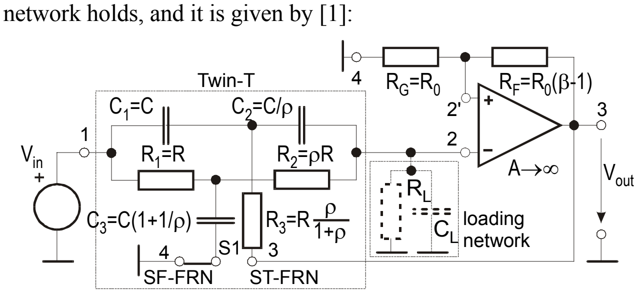

Figure 6. 2nd-order BR active-RC filter of class-4: "Split Feedback Twin-T" section as in [3].

$$R_3/C_3 = R_p/C_p\,. \tag{20}$$

Introducing the impedance-scaling factor ρ, to obtain the potentially symmetrical twin-T, into (17), i.e.

$$R_1=R;\ C_1=C;\ R_2=\rho R;\ C_2=C/\rho;\ R_3=\rho R/(1+\rho);\ C_3=C(\rho+1)/\rho \tag{21}$$

we satisfy (20) and obtain the following simple relations:

$$\omega_p=\omega_z=\frac{1}{RC}\,;\ q_z=\infty;\ q_p=\hat{q}\cdot\frac{1}{1-\beta/2}\,;\ \hat{q}_{\text{Twin-T}}=\frac{1}{2}\cdot\frac{\rho}{1+\rho}\,. \tag{22}$$

Note that the impedance-scaling factor ρ exists only in equation for calculating $\hat{q}$. If we increase $\rho\to\infty$, the passive pole Q, $\hat{q}\to 0.5$.

The process of deriving a potentially symmetrical twin-T network [1][4] is identical as for the bridged-T network presented above. It is actually a third-order network but because of (20) the negative real pole and zero are cancelled out. Therefore the twin-T passive network provides a 2nd-order transfer function of the form given by:

$$\hat{t}_{12}(s)=\frac{V_2}{V_1}=k_{12}\frac{s^2+\omega_z^2}{s^2+(\omega_p/\hat{q})\cdot s+\omega_0^2}\,, \tag{23}$$

For the symmetrical case with ρ=1, the parameters in (23) take on the values in (22), and $k_{12}=1$, $\hat{q}=1/4$.

It is well known [1] that the network in the positive feedback loop of the class-4 circuit has a BP characteristic of the form:

$$\hat{t}_{32}(s)=\frac{V_2}{V_3}=1-\hat{t}_{12}(s)=\frac{\omega_k\cdot s}{s^2+(\omega_0/\hat{q})\cdot s+\omega_0^2} \tag{24}$$

and therefore the pole parameters in (16) have the form:

$$\omega_p=\omega_0\,;\ q_p=\hat{q}\cdot(1-i\cdot\beta\hat{q}\omega_k/\omega_0)^{-1}\,, \tag{25}$$

where i=1 or 0.5 [we have β or β/2 in (25)] for ST-and SF-FRN, respectively. Note that ω_p is independent of β, and q_p has the form presented in (9). Thus the relative sensitivity of the pole Q, q_p to the variations of gain β, $S_\beta^{q_p}$ has the form given by (10) above (with β instead $\overline{\beta}$). Furthermore, from (18) the sensitivity of the gain β to the R_F and R_G follows (in class-4) and it is given by:

$$S_{R_F}^{\beta}=-S_{R_G}^{\beta}=1-1/\beta\,. \tag{26}$$

With a potentially symmetrical twin-T network ST-FRN has the gain 2β in (17) and (22) instead of β, and the other expressions in (17) apply. Generally, from (25) and (26) we calculate the relative sensitivity of the pole Q, q_p to R_F and R_G, and it is given by:

$$S_{R_F}^{q_p}=-S_{R_G}^{q_p}=S_\beta^{q_p}\cdot S_{R_F}^{\beta}=q_p\cdot(\hat{q}^{-1}-i\cdot\omega_k/\omega_0)-1\,, \tag{27}$$

where i=1 or 0.5. From (22) and (25) and with i=0.5 we have $\omega_k/\omega_0=1/\hat{q}$; for the special case SF-FRN we can rewrite (27) into:

$$S_{R_F}^{q_p}=-S_{R_G}^{q_p}=0.5\cdot q_p/\hat{q}-1\,. \tag{28}$$

Unlike in (13), note that the q_p sensitivities to resistors R_G and R_F in (28) are inversely proportional to the passive pole Q, $\hat{q}$ value. The reason for this lies in the different techniques of obtaining pole Q values for class-3 and class-4 networks given above. Thus the decrease of sensitivity in (10) will reduce the sensitivity to the feedback-resistor tolerances in the case of class-4 networks. Both sensitivities in (13) and (28) are proportional to the pole Q, q_p which is the characteristic of "medium-Q" filters [3].

Furthermore, it has been investigated using the program "Mathematica", and the results of this investigation show that increasing the scaling factor ρ will also decrease the coefficient a_1 sensitivities to the passive components R_i and C_i (i=1,2,3).

To double-check the above conclusions we designed the filter in Fig. 6, with two values of ρ for the BR example above. The resulting filters are in Table 4 and corresponding MC runs are in Fig. 7. Note that in the second column in Fig. 7 we perform only variation of feedback resistors R_G and R_F.

TABLE IV. COMPONENT VALUES OF 2ND-ORDER BR FILTERS WITH POTENTIALLY SYMMETRICAL TWIN-T.

No.	ρ	R_1	R_2	R_3	C_1	C_2	C_3	β	$\hat{q}$
1)	1	15.9	15.9	7.95	10	10	20	1.90	0.25
2)	4	15.9	63.6	12.7	10	2.5	12.5	1.84	0.40

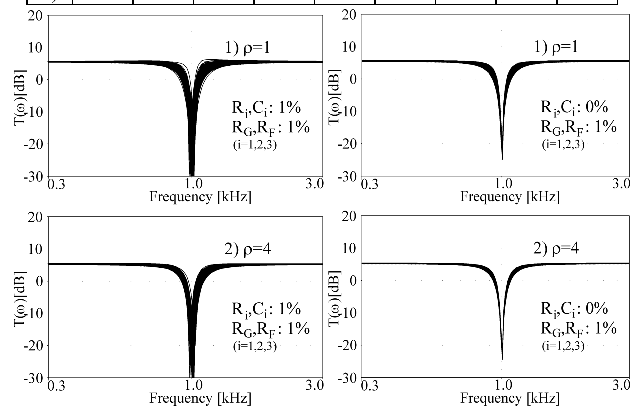

Figure 7. Monte Carlo runs of impedance-tapered 2nd-order BR filters given in Table 4.

Clearly, as ρ increases, the sensitivities in Fig. 7 are improving. We can conclude that: *we should enlarge the design factor ρ in (22) in the design procedure for class-4 filters*.

V. CONCLUSIONS

In this paper we described the design procedure of the active-RC filters, which have a symmetrical bridged-T and twin-T networks in negative (class-3) and positive (class-4) feedback loops. The process of deriving "potentially symmetrical" networks by increasing the impedance of one half of those symmetrical networks ρ times, has been described in [1][4]. Choosing a scaling factor ρ>1 the passive pole Q factor, $\hat{q}$ of both networks is increased. It is shown that for class-4 filters (Twin-T BR filter) the passive sensitivity can be reduced choosing larger ρ (and consequently larger $\hat{q}$). For the class-3 filters (Deliyannis BP section) the passive sensitivity can only be reduced by increasing the q_z value of bridged-T, even though the $\hat{q}$ is thereby decreased. For the latter it is optimal to choose resistive impedance tapering with either equal capacitors or capacitors selected for GSP-minimization [5].

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